

Accurate and Efficient Parametric Macromodeling of IC Drivers via Sigmoidal Basis Functions

Original

Accurate and Efficient Parametric Macromodeling of IC Drivers via Sigmoidal Basis Functions / Stievano, IGOR SIMONE; Maio, Ivano Adolfo; Canavero, Flavio. - STAMPA. - (2003), pp. 57-60. (7th IEEE Workshop on Signal Propagation on Interconnects (SPI) Siena (Italy) May 11-14, 2003).

Availability:

This version is available at: 11583/1409393 since:

Publisher:

Piscataway, N.J. : IEEE

Published

DOI:

Terms of use:

This article is made available under terms and conditions as specified in the corresponding bibliographic description in the repository

Publisher copyright

(Article begins on next page)

Accurate and Efficient Parametric Macromodeling of IC Drivers via Sigmoidal Basis Functions

I.S. Stievano, I.A. Maio, F.G. Canavero
 Politecnico di Torino - Dipartimento di Elettronica
 C.so Duca degli Abruzzi, 24, 10129, Torino, Italy
 {stievano,maio,canavero}@polito.it

Abstract

This paper addresses the selection of parametric relations for the macromodeling of the output and power supply ports of IC output buffers. Relations defined by sigmoidal functions and parameter estimation via fully nonlinear optimization algorithms can lead to models with improved efficiency. Modeling examples involving commercial devices are shown.

1 Introduction

The system level simulation of high performance digital circuits for signal integrity (SI) and electromagnetic compatibility (EMC) effects requires effective models of the Integrated Circuits (ICs) ports driving and loading interconnect structures.

Recently, a macromodeling methodology based on the estimation of parametric models from port transient responses has been proposed and successfully applied to real modeling problems [1, 2, 3]. This approach has specific advantages, making it a useful complement to the traditional modeling approach based on simplified equivalent circuits of the device ports [4].

This paper addresses the choice of the parametric relation for the modeling of the output and power supply ports of IC drivers. Parametric relations defined by Gaussian Radial Basis Functions (RBF) and by sigmoidal (SIG) functions are exploited along with different algorithms for the estimation of model parameters. Such relations are applied to the modeling of IBM commercial drivers and their performance are tested for realistic simulation problems.

2 Parametric macromodeling overview

The modeling of ICs for SI and EMC simulations amounts to finding suitable port relationships (which we refer to as “constitutive”), for a known logical activity of the ICs. As an example, Fig. 1 shows the typical structure of an IC output buffer (driver in the following) that can be considered as a three-port element, whose input port is connected to the IC internal logic and the other two ports are the output and the power supply ports connected to the external interconnects. The electrical behavior of output and power supply ports for such element can be described by the following constitutive relations

$$\begin{cases} i &= F_o(v, v_{dd}) \\ i_{dd} &= F_d(v, v_{dd}) \end{cases} \quad (1)$$

where F_o and F_d are suitable nonlinear dynamic operators.

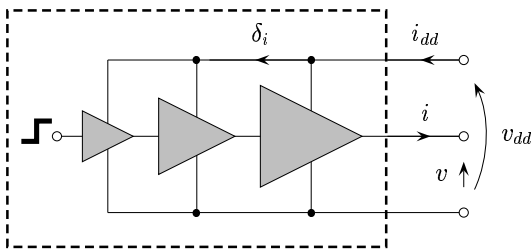


Figure 1: General structure of a driver circuit and its relevant (output and power supply) port electric variables.

For parametric macromodeling, the above constitutive relations are

sought as dynamic nonlinear parametric equations. The use of parametric equations to model physical systems is conceptually simple and can be described by the three steps: (1) *model selection*, *i.e.*, the selection of the parametric relation defining the model (model representation hereafter); (2) *parameter estimation*, *i.e.*, the computation of the model parameter values so that the model responses mimic well those of the device under modeling; (3) *model implementation*, *i.e.*, the translation of the model in a circuit simulation environment by representing its equations with equivalent circuits.

Model selection is the most critical step of the modeling process, since a model representation far from the functional form of the real system can hardly reproduce its behavior. The model representation suitable for buffer circuits is searched for within the class of discrete-time parametric models. This is mainly due to the large availability of methods for the estimation of this class of models [5, 6]. Besides, this is the natural choice when the raw data, *i.e.*, the external responses of the system, are known as sampled waveforms. An additional back conversion to continuous-time is needed for the implementation of the model as a subcircuit, yet this is easily carried out via standard methods in step three of the modeling procedure [1].

A general discrete-time input/output parametric relation can be obtained by a nonlinear mapping defined by a sum of basis functions [6]. For a single input (extension to multiple input is straightforward) this writes

$$y(k) = g(\mathbf{x}(k), \Theta) \quad (2)$$

where y is the output, vector Θ collects the model parameters and the scalar function g maps the present and past samples of the input u and the past samples of the output into the present sample of the output. The mapped input/output samples are collected in the regressor vector

$$\mathbf{x}(k) = [u(k), u(k-1), \dots, u(k-r), y(k-1), \dots, y(k-r)]^T \quad (3)$$

where index r is referred to as the dynamic order of the model. Function g is defined by

$$g(\varphi, \Theta) = \sum_{n=1}^p \alpha_n \phi_n(\eta(\mathbf{x})) \quad (4)$$

where ϕ_n is the n -th basis function, obtained from a single mother generating function $\phi(\eta)$ by changing its spreading and its position (nonlinear parameters), α_n is a linear coefficient (linear parameter) and p is the total number of components (model size). Many different basis functions can be used in (4), giving rise to model representations with significantly different properties.

Parameter estimation relies on the information contained in a set of transient responses (*identification signals* hereafter) of the system under modeling $\{u(k), y(k)\}$, $k = 1 \dots N$, where N is the length of the sequences. For given values of the model size p and of the dynamic order r , model parameters are computed as solution of the following nonlinear approximation problem, usually cast as a least square problem

$$\mathbf{U} = \begin{bmatrix} u(1) \\ \vdots \\ u(N) \end{bmatrix} \approx \mathbf{g}(\mathbf{X}, \Theta) = \begin{bmatrix} g(\mathbf{x}(1), \Theta) \\ \vdots \\ g(\mathbf{x}(N), \Theta) \end{bmatrix} \quad (5)$$

Specific algorithms are available to solve this problem, that depends on the specific choice of the family of basis functions [6].

3 Basis functions and estimation algorithms

Presently, parametric macromodels based on Gaussian RBF expansions have been successfully applied so far to the macromodeling of the ports of digital ICs [1, 2, 3]. Gaussian RBF models belong to the generic class defined by (4), where the mother generating function is $\phi(\eta) = \exp(-\eta^2/2)$ and the n -th basis function ϕ_n is defined by the argument

$$\eta(\mathbf{x}) = \|\mathbf{x}(k) - \mathbf{c}_n\|/\beta_n \quad (6)$$

where $\|\cdot\|$ denotes the Euclidean norm and \mathbf{c}_n and β_n are the nonlinear parameters defining the shape factor of the n -th basis function.

Gaussian RBF models offer remarkable advantages. Mainly, they are robust and have a regular and smooth behavior outside the fitting domain. The estimation of model parameters relies on simple and efficient algorithms [7, 8] in which the nonlinear least squares problem (5) is cast as an equivalent linear problem. This can be done since RBF models are weakly sensitive to the position of center and spreading parameters. In such a way, the set of possible center and spreading parameters are selected *a priori* and the nonlinear problem (5) is reduced to the estimation of the linear parameters only.

However, this is not the only choice of basis functions leading to models suitable for the approximation of a wide class of nonlinear dynamic systems. A complete overview of possible choices can be found in [6]. An alternate choice considered in this paper is the widely used class of SIG basis functions that are defined by a mother function $\phi(\eta) = \tanh(\eta)$ and by

$$\eta(\mathbf{x}) = \mathbf{v}_n^T \mathbf{x}(k) + b_n \quad (7)$$

where \mathbf{v}_n and b_n are the nonlinear parameters of the basis function ϕ_n .

It is worth noting that, Gaussian RBF have spherical symmetry and finite spreading, whereas sigmoidal functions defined by (7) have planar symmetry and unbounded support. The planar symmetry is more suitable for fitting the actual constitutive relations of output and power supply ports of IC drivers. Thereby, (7) is a good alternative to Gaussian RBF for the problem at hand, leading to models with improved efficiency (less basis functions). Besides, for the approximation of mappings that exhibit a regular (*e.g.*, weakly nonlinear) behavior, Gaussian RBF representations can lead to models with a large number of basis functions. As an example, Fig. 2 shows the approximation of a one dimensional static mapping by the superposition of Gaussian bell shaped functions and of sigmoid functions within a specific domain.

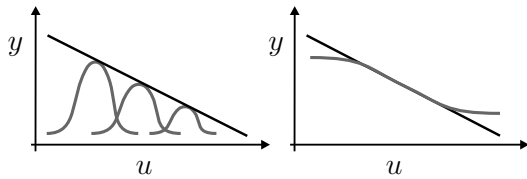


Figure 2: Approximation of a simple linear static $u - y$ relation by the superposition of different scalar basis functions (left panel: Gaussian bells; right panel: sigmoid)

Unfortunately, SIG-type models do not exhibit the nice property of weak sensitivity to the nonlinear parameters and therefore a fully nonlinear estimation algorithm is required to solve problem (5). Within the many possible estimation algorithms we found good results with the Levenberg-Marquardt method [10] and the procedure for the selection of the initial guess of parameters in [9].

As a final remark, supplemental information on the device being modeled, like its static characteristic $\{u_{sc}, y_{sc}\}$, when available, can

be included in the model. This can be done by modifying the least squares problem (5) by stacking additional rows as follows,

$$\begin{bmatrix} \mathbf{U} \\ \mathbf{U}_{sc} \end{bmatrix} \begin{bmatrix} \mathbf{g}(\mathbf{X}, \Theta) \\ \mathbf{g}(\mathbf{X}_{sc}, \Theta) \end{bmatrix} \quad (8)$$

where \mathbf{U}_{sc} is a column vector collecting the static values of the input variable $[u_{sc}(1), u_{sc}(2), \dots]$, and \mathbf{X}_{sc} collects the regressor vectors built on the static characteristic (the present and past values of u and the past values of y in the regressor vector (3) are set to the same static values in $\{u_{sc}, y_{sc}\}$). The range of the static characteristic is usually chosen larger than the range explored by the transient input identification sequence stored in \mathbf{U} , ensuring the right static behavior over a wide domain.

4 Output and power supply port macromodels

This Section shortly reviews macromodels for output and power supply ports of driver circuits. The key problem for the development of a driver model is that the internal (logic) signal feeding the buffer is not a measurable quantity. In spite of this, the port model must allow for variation of the logic state. For constant values of the power supply port voltage, a parametric macromodel of the output port has been presented and thoroughly discussed in [1]. It approximates the output port constitutive relation with a two-piece model

$$i(k) = w_1(k)f_1(\Theta_1, v) + w_2(k)f_2(\Theta_2, v) \quad (9)$$

where f_1 and f_2 are nonlinear parametric models accounting for the port behavior in a fixed High or Low logic state, respectively and w_1 and w_2 are time-varying weighting coefficients for state switchings.

In order to include the effects of the power supply voltage v_{dd} in the macromodel (9), taking into account supply voltage fluctuations on the switching of logic devices, the v_{dd} variable is added as an additional input in the parametric models f_1 and f_2 . The output port macromodel then writes

$$i(k) = w_1(k)f_1(\Theta_1, v, v_{dd}) + w_2(k)f_2(\Theta_2, v, v_{dd}) \quad (10)$$

The weighting coefficients describing state switching, instead, are constant with respect to v_{dd} owing to the properties of model representation (9) [1]. The transient responses for the estimation of the model parameters are obtained by driving the model devices with $v(k)$ and $v_{dd}(k)$ signals that are multilevel noisy waveforms [5].

The models of the power supply ports are needed for the simulation of switching noise effects and yield the driver supply current i_{dd} as a function of the supply port voltage v_{dd} and of the output port voltage v (see Fig. 1). The model representation exploited for the power supply port of drivers is

$$i_{dd}(k) = w_{d1}(k)f_{d1}(\Theta_{d1}, v, v_{dd}) + w_{d2}(k)f_{d2}(\Theta_{d2}, v, v_{dd}) + \delta_i(k) \quad (11)$$

where $\delta_i(k)$ takes into account the supply current drawn by the driver stages that precede the last one, and f_{d1} and f_{d2} are the parametric submodels of the current of the last driver stage when it operates in the LOW and HIGH logic states, respectively, and w_{d1} and w_{d2} are the usual weighting coefficients describing state switchings.

5 Numerical examples

In this Section, the parametric models of Section 4 with the basis functions described in Section 3 are applied to the modeling of commercial drivers. In the following, RBF and SIG indicate models composed of Gaussian RBF and of sigmoid functions, respectively, whereas SIG-SC denote models composed by sigmoid functions whose parameters are estimated by including information on the static characteristics, as shown in Section 3. All models are obtained from

Table 1: Mean Square Error (MSE) between the output identification sequence and the model response to the identification sequences (approximation error). Both the RBF and the SIG type models are considered. The total number of basis functions p included in the models is in the range $[1, 10]$.

p	MSE(RBF)	MSE(SIG)
1	4.12e-1	2.07e-6
2	7.22e-2	8.30e-7
3	3.25e-4	8.28e-7
4	3.14e-4	8.11e-7
5	1.40e-4	8.78e-7
6	2.40e-5	8.48e-7
7	1.63e-6	8.87e-7
8	1.59e-6	8.82e-7
9	1.44e-6	8.88e-7
10	1.34e-6	8.65e-7

transient responses of detailed transistor-level model of the devices under modeling (hereafter references) and implemented as SPICE subcircuits. Reference and models are compared by simulating realistic test circuits.

Example #1. The first modeled device is the output port of a high-speed IBM CMOS driver ($V_{dd} = 1.8$ V) for servers operating at 250 MHz. For this device, both the complete RBF and the SIG type macromodels are estimated. For this example, we concentrate on the characterization of the output port only and assume constant power supply voltage equal to the nominal value V_{dd} .

As a first comparison, devised to highlight the differences among the possible choices of basis functions, both the RBF and the SIG parametric models are estimated for submodel f_1 of (10), *i.e.*, the dynamic $i - v$ port relation when the driver is forced in the fixed High output state. In this example, the dynamic order of submodels is $r = 1$.

Table 1 shows the Mean Square Errors (MSE) computed during the estimation procedure for submodel f_1 and different values of the number of basis functions p included in the model. MSE values on the order of $1E-6$ lead to macromodels reproducing the behavior of the device very well and make the predicted responses almost indistinguishable from the reference ones. It is worth noting that the same good accuracy obtained with RBF models for $p = 7$ is achieved with SIG-type models for $p = 1$, only.

The complete macromodel (10) is estimated using the procedure detailed in [1] and Table 2 summarizes some results on the complexity and efficiency of possible macromodels. For this comparison, the RBF, SIG and SIG-SC type of parametric models are used. The table lists the number of basis functions p_1 and p_2 , for the submodels f_1 and f_2 , respectively, and the CPU time required to compute a simple transient simulation test using the reference transistor-level models and two SPICE-like implementations of the macromodels. The test setup consists of the driver being modeled connected to a 100Ω load resistor and producing a logic high pulse (bit pattern "010"). The speed-up factor introduced by the macromodels can be clearly appreciated.

As a realistic validation setup, the example driver #1 applying a logic high pulse on an open-ended ideal transmission line ($Z_0 = 100 \Omega$, $T_d = 100$ ns) is considered. Fig. 3 shows the near-end transient voltage waveform computed through PowerSPICE and using the reference transistor-level model and the SIG-SC type macromodel. Curves obtained using the RBF and the SIG type of models are not reported, since they are indistinguishable from that of the SIG-SC type.

An additional index on the model quality is obtained by computing the timing error, that is expressed as the maximum delay between the

Table 2: Number of basis functions of the possible macromodels of the example driver #1 and CPU time comparison for a simple transient simulation test (see text).

Macromodel	p_1	p_2	CPU time (PowerSPICE)	CPU time (Pspice)
reference	-	-	27 s	-
RBF	7	8	0.42 s	1.77 s
SIG	1	2	0.22 s	0.50 s
SIG-SC	3	3	0.30 s	0.80 s

reference and the macromodel responses measured for a suitable voltage crossing (*e.g.*, 50 % of the voltage swing). As an example, for the curves of Fig. 3 the timing error is 7 ps (0.35 % of the bit time).

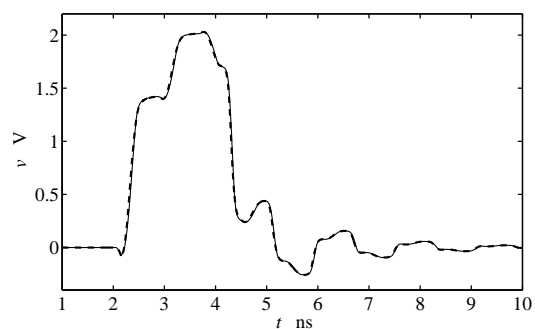


Figure 3: Near-end voltage waveform on an ideal transmission line driven by the example driver #1 (see text). Solid line: reference; dashed line: SIG-SC macromodel.

Example #2. The modeled device is a high-speed IBM CMOS driver ($V_{dd} = 1.32$ V) for servers operating at 500 MHz. For this device, both the output and the power supply port macromodels are estimated. In this example, only the SIG-SC type parametric models are considered.

The obtained output port macromodel (10) turns out to have submodels f_1 and f_2 composed of 8 and 11 basis functions, respectively. Whereas, the power supply port macromodel (11) has submodels f_{d1} and f_{d2} composed of 9 and 5 functions, respectively. All the submodels have dynamic order $r = 2$.

As a first validation test, Fig. 4 shows the driver port waveforms predicted by the reference transistor-level model of the device and by the macromodels while the driver applies a bit stream "0100110010" on a dynamic load (ideal transmission line with $Z_0 = 50 \Omega$ and 0.3 ns) and the power supply pin is connected to a V_{dd} battery. The timing error for this test is 11 ps (1.1 % of the bit time).

A second validation setup for a Simultaneous Switching Noise (SSN) prediction is considered. It is composed of M identical open-ended transmission lines driven by M replicas of the modeled device. The power supply port of every driver is connected to a common power supply structure that is modeled by R_s , L_d and by the battery V_{dd} . The parameter values are: transmission line characteristic impedance $Z_0 = 50 \Omega$, time delay $T_d = 0.3$ ns; $R_s = 1$ m Ω , $L_d = 0.1$ nH and $V_{dd} = 1.32$ V. All drivers are then driven to switch simultaneously (bit stream "0100110010") and the circuit waveforms are computed.

Figure 5 shows the comparison between the reference and the predicted voltage and current waveforms at the output of a driver and the total power supply voltage and current waveforms for $M = 11$ simultaneous switchings. The model predictions and the reference responses are in good agreement. The parametric model involved in this test has been estimated for v_{dd} variations in the range $V_{dd} \pm 15\%$, whereas the

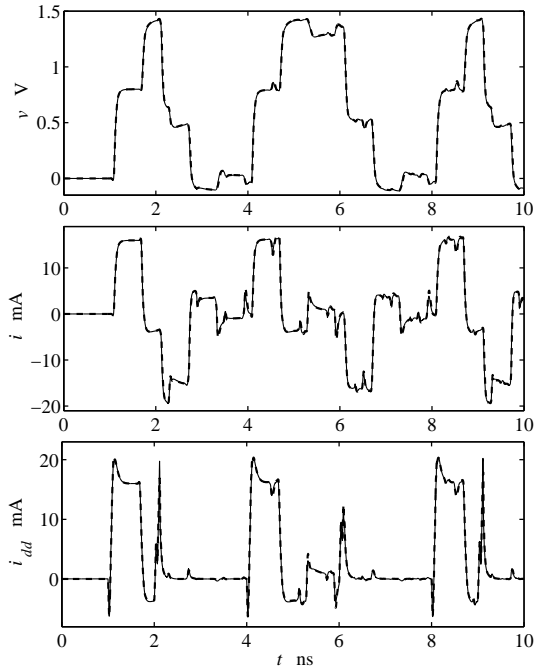


Figure 4: Near-end voltage waveform on an ideal transmission line driven by the example driver #2 whose power supply pin is connected to a V_{dd} battery (see text). Solid line: reference; dashed line: SIG-SC macromodel.

v_{dd} variations for this case exceeds the modeling range. This means that the accuracy of the obtained model remains acceptable also on the boundaries of the v_{dd} modeling range. The timing error computed from the previous curves is 31 ps (3.1 % of the bit time)..

6 Conclusions

The parametric approach discussed in this paper offers a rigorous framework for the modeling of nonlinear dynamic devices from external responses. The use of RBF model representations allows to handle most devices and produces model with good efficiency and accuracy. However, when more information on the device properties is exploited, specific choices of basis functions (sigmoidal class and ridge construction) and estimation algorithms can lead to improved models. The advantages of the proposed modeling strategies are demonstrated for the output and power supply ports of driver circuits, obtaining accurate and efficient macromodels that can be effectively used in actual simulation problems.

Acknowledgements

The Authors wish to acknowledge many helpful discussion and exchanges with G. Katopis and Z. Chen of IBM, Enterprise System Group, NY, USA. This work was supported in part under PRIN grant #2002093437 and CERCOM.

References

- [1] I. S. Stievano, F. G. Canavero, I. A. Maio, "Parametric Macromodels of Digital I/O Ports," *IEEE Transactions on Advanced Packaging*, Vol. 25, No. 2, pp. 255–264, May 2002.
- [2] F. G. Canavero, I. A. Maio, I. S. Stievano "M π log, Macromodeling via Parametric Identification of Logic Gates," *Proc. of 4th Annual Austin IBM CAS Conference*, Austin, TX, Feb. 21, 2003.
- [3] I. S. Stievano, I. A. Maio, F. G. Canavero, "Behavioral Models of I/O Ports from Measured Transient Waveforms," *IEEE Transactions on Instrumentation and Measurement*, Vol. 51, No. 6, pp. 1266–1270, Dec. 2002.

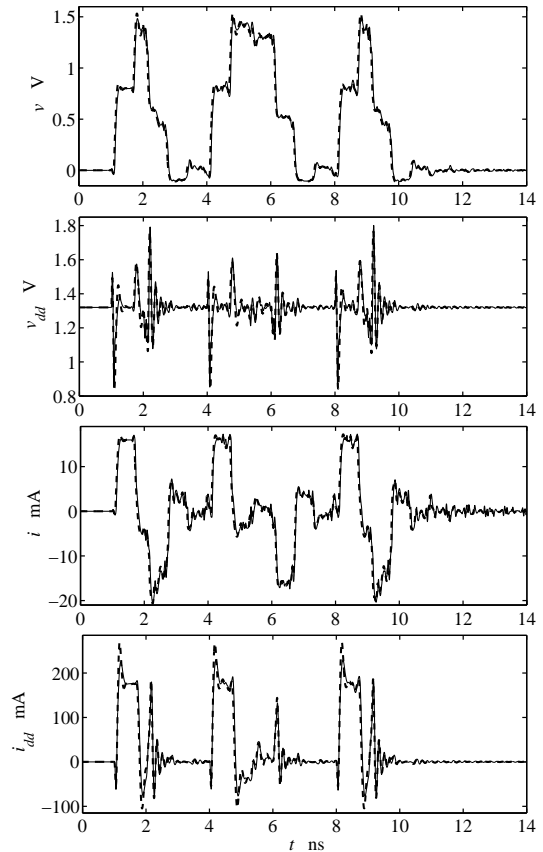


Figure 5: Voltage and current waveforms at the output of a driver and the total power supply voltage and current waveforms for $M = 11$ simultaneous switchings.

- [4] "I/O Buffer Information Specification (IBIS) Ver. 3.2," on the web at <http://www.eigroup.org/ibis/ibis.htm>, Sep. 1999.
- [5] L. Ljung, *System identification: theory for the user*, Prentice-Hall, 1987.
- [6] J. Sjöberg et al., "Nonlinear black-box modeling in system identification: a unified overview," *Automatica*, Vol. 31, No. 12, pp. 1691–1724, 1995.
- [7] S. Chen, C. F. N. Cowan and P. M. Grant, "Orthogonal least squares learning algorithm for radial basis function network," *IEEE Transactions on Neural Networks*, Vol. 2, No. 2, pp. 302–309, Mar. 1991.
- [8] K. Judd and A. Mees, "On selecting models for nonlinear time series," *Physica D*, Vol. 82, pp. 426–444, 1995.
- [9] D. Nguyen, B. Widrow, "Improving the learning speed of 2-layer neural networks by choosing initial values of the adaptive weights," *Proc. of the International Joint Conference on Neural Networks (IJCNN)*, San Diego, CA, USA, pp. 21–26, Jun. 17–21, 1990.
- [10] M. T. Hagan, M. Menhaj, "Training feedforward networks with the marquardt algorithm," *IEEE Transactions on Neural Networks*, Vol. 5, N. 6, pp. 989–993, Nov. 1994.